

GRAB-N-PULL: AN OPTIMIZATION FRAMEWORK FOR FAIRNESS-ACHIEVING NETWORKS

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ABSTRACT

In this paper, we present an optimization framework for designing precoding (a.k.a. beamforming) signals that are instrumental in achieving a fair user performance through the networks. The precoding design problem in such scenarios can typically be formulated as a non-convex max-min fractional quadratic program. Using a penalized version of the original design problem, we derive a simplified quadratic reformulation of the problem in terms of the signal (to be designed). Each iteration of the proposed design framework consists of a combination of power method-like iterations and the Gram-Schmidt process, and as a result, enjoys a low computational cost. Moreover, the suggested approach can handle various types of signal constraints such as total-power, per-antenna power, unimodularity, or discrete-phase requirements—an advantage which is not shared by other existing approaches in the literature.

Index Terms— Beamforming, fractional programming, max-min fairness, non-convex optimization, precoding

1. INTRODUCTION

A widely used proactive interpretation of fairness in wireless networks, referred to as the *max-min* fairness [1–8], is to allocate the available resources in order to maximize the minimal user performance in the network. In such scenarios, a judicious design of the *precoding* signals for different users can be viewed as a vital part of the network configuration.

1.1. Problem Formulation

We consider the precoding problem for a downlink channel, with an M -antenna transmitter and K single-antenna users. Let $\mathbf{h}_i \in \mathbb{C}^M$ denote the channel between the transmit antennas and the i^{th} user. Also let $\mathbf{w}_i \in \mathbb{C}^M$ denote the *precoding* vector corresponding to the i^{th} user. To form the data stream to the users, any complex symbol to be transmitted, will be modulated by the precoding vector of the intended user. The precoding vectors are to be designed in order to enhance the network performance. In particular, the signal-to-noise-plus-interference ratio (SINR) of the i^{th} user is given by [9]

$$\text{SINR}_i = \frac{\mathbf{w}_i^H \mathbf{R}_i \mathbf{w}_i}{\left(\sum_{j \in [K] \setminus \{i\}} \mathbf{w}_j^H \mathbf{R}_i \mathbf{w}_j \right) + \sigma_i^2}, \quad \forall i \in [K], \quad (1)$$

where $\mathbf{R}_i = \mathbb{E}\{\mathbf{h}_i \mathbf{h}_i^H\}$ is the covariance matrix of the i^{th} channel, σ_i^2 denotes the variance of the zero-mean additive white Gaussian

noise (AWGN), and $[K] = \{1, 2, \dots, K\}$. Note that by a specific reformulation, the SINR metric in (1) can be rewritten as a fractional quadratic criterion. To see this, define the *stacked* precoding vector $\mathbf{w} \in \mathbb{C}^N$ (with $N = KM$) as

$$\mathbf{w} \triangleq \text{vec}([\mathbf{w}_1 \ \mathbf{w}_2 \ \dots \ \mathbf{w}_K]), \quad (2)$$

and observe that (1) will increase for any increased scaling of \mathbf{w} . As a result, any finite-energy constraint on \mathbf{w} while maximizing $\{\text{SINR}_i\}$ will be *active*, i.e. it will be satisfied with equality. Accordingly, suppose $\|\mathbf{w}\|_2^2 = P$, and let

$$\mathbf{A}_i \triangleq \mathbf{R}_i \otimes \mathbf{Diag}(\mathbf{e}_i), \quad \forall i \in [K], \quad (3)$$

$$\mathbf{B}_i \triangleq \mathbf{R}_i \otimes (\mathbf{I}_K - \mathbf{Diag}(\mathbf{e}_i)) + \frac{\sigma_i^2}{P} \mathbf{I}_N, \quad \forall i \in [K], \quad (4)$$

where $\mathbf{Diag}(\cdot)$ denotes the diagonal matrix formed by the entries of the vector argument, \otimes stands for the Kronecker product of matrices, and \mathbf{e}_i is the i^{th} standard basis vector in \mathbb{C}^K . Now, it is not difficult to verify that

$$\text{SINR}_i = \frac{\mathbf{w}^H \mathbf{A}_i \mathbf{w}}{\mathbf{w}^H \mathbf{B}_i \mathbf{w}}, \quad \forall i \in [K], \quad (5)$$

in which $\{\mathbf{A}_i\}$ are positive semidefinite (PSD) and $\{\mathbf{B}_i\}$ are positive definite (PD). Finally, the precoding design problem for maximizing the minimal user SINR performance can be formulated as

$$\begin{aligned} \mathcal{P}_1 : \max_{\mathbf{w}} \quad & \min_{i \in [K]} \left\{ \frac{\mathbf{w}^H \mathbf{A}_i \mathbf{w}}{\mathbf{w}^H \mathbf{B}_i \mathbf{w}} \right\} \\ \text{s. t.} \quad & \mathbf{w} \in \Omega, \end{aligned} \quad (6)$$

where Ω denotes the feasible set of \mathbf{w} determined by the associated signal constraints. Note that \mathcal{P}_1 may also be used to formulate the weighted SINR optimization problems; see [1, 2] for details.

1.2. Contributions of this Work

The above precoding design problem has been studied extensively in the literature when Ω denotes a total-power or per-antenna power constraint (see e.g., [1–8] and the references therein). As a result, different approaches have been proposed to solve the design problem, including those based on uplink-downlink duality [1], the Lagrangian duality [3] and quasi-convex formulations [8].

In this work, we propose a novel optimization framework (which we call Grab-n-Pull) that can efficiently tackle \mathcal{P}_1 . Note that the proposed framework subsumes the traditional total-power or per-antenna power constraints, while also allowing for intricate signal constraints such as unimodularity or discrete-phase requirements.

Remark 1: It is worth mentioning that the problem formulation \mathcal{P}_1 in (6) is also useful in other applications, including e.g., waveform design for radar [10, 11], and relay beamforming [12, 13]. ■

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2. THE PROPOSED FRAMEWORK

We begin by considering a reformulated version of \mathcal{P}_1 ; namely,

$$\mathcal{P}_2 : \quad \max_{\mathbf{w}} \quad \min_{i \in [K]} \{\lambda_i\} \\ \text{s. t.} \quad \mathbf{w} \in \Omega, \quad (7)$$

$$\lambda_i = \frac{\mathbf{w}^H \mathbf{A}_i \mathbf{w}}{\mathbf{w}^H \mathbf{B}_i \mathbf{w}}, \quad \forall i \in [K]. \quad (8)$$

Note that (8) holds if and only if $\|\mathbf{A}_i^{\frac{1}{2}} \mathbf{w}\|_2^2 = \lambda_i \|\mathbf{B}_i^{\frac{1}{2}} \mathbf{w}\|_2^2$, or equivalently $\|\mathbf{A}_i^{\frac{1}{2}} \mathbf{w}\|_2 = \sqrt{\lambda_i} \|\mathbf{B}_i^{\frac{1}{2}} \mathbf{w}\|_2$, where $(\cdot)^{\frac{1}{2}}$ denotes the Hermitian square-root of the matrix argument [14]. In particular, the left-hand side of (8) is *close* to the right-hand side of (8) if and only if $\|\mathbf{A}_i^{\frac{1}{2}} \mathbf{w}\|_2$ is *close* to $\sqrt{\lambda_i} \|\mathbf{B}_i^{\frac{1}{2}} \mathbf{w}\|_2$. Therefore, by employing the auxiliary variables $\{\lambda_i\}$, one can consider the following optimization problem as an alternative to \mathcal{P}_2 (and \mathcal{P}_1):

$$\mathcal{P}_3 : \quad \max_{\mathbf{w}, \{\lambda_i\}} \quad \min_{i \in [K]} \{\lambda_i\} - \eta \sum_{i=1}^K (\|\mathbf{A}_i^{\frac{1}{2}} \mathbf{w}\|_2 - \sqrt{\lambda_i} \|\mathbf{B}_i^{\frac{1}{2}} \mathbf{w}\|_2)^2 \\ \text{s. t.} \quad \mathbf{w} \in \Omega; \lambda_i \geq 0, \quad \forall i \in [K]; \quad (9)$$

in which $\eta > 0$ determines the weight of the penalty-term added to the original objective of \mathcal{P}_2 ; and where \mathcal{P}_3 and \mathcal{P}_2 coincide as $\eta \rightarrow +\infty$. Note that optimizing \mathcal{P}_3 with respect to (w. r. t.) \mathbf{w} may require rewriting \mathcal{P}_3 as a quartic objective in \mathbf{w} . To circumvent this, we continue by introducing \mathcal{P}_4 —yet another alternative objective:

$$\mathcal{P}_4 : \quad \max_{\mathbf{w}, \{\lambda_i\}, \{\mathbf{Q}_i\}} \quad \min_{i \in [K]} \{\lambda_i\} - \eta \sum_{i=1}^K \|\mathbf{A}_i^{\frac{1}{2}} \mathbf{w} - \sqrt{\lambda_i} \mathbf{Q}_i \mathbf{B}_i^{\frac{1}{2}} \mathbf{w}\|_2^2 \\ \text{s. t.} \quad \mathbf{w} \in \Omega, \lambda_i \geq 0, \quad \forall i \in [K]; \quad (10)$$

$$\mathbf{Q}_i^H \mathbf{Q}_i = \mathbf{I}_N, \quad \forall i \in [K]. \quad (11)$$

Towards understanding the equivalence of \mathcal{P}_3 and \mathcal{P}_4 , observe that the maximizer \mathbf{Q}_i of \mathcal{P}_4 is a unitary *rotation* matrix that aligns the vector $\mathbf{B}_i^{\frac{1}{2}} \mathbf{w}$ in the same *direction* as $\mathbf{A}_i^{\frac{1}{2}} \mathbf{w}$, without changing its ℓ_2 -norm (i.e. $\|\mathbf{B}_i^{\frac{1}{2}} \mathbf{w}\|_2$). More precisely, at the maximizer \mathbf{Q}_i of \mathcal{P}_4 , we have that

$$\mathbf{Q}_i \mathbf{B}_i^{\frac{1}{2}} \mathbf{w} = \left(\frac{\|\mathbf{B}_i^{\frac{1}{2}} \mathbf{w}\|_2}{\|\mathbf{A}_i^{\frac{1}{2}} \mathbf{w}\|_2} \right) \mathbf{A}_i^{\frac{1}{2}} \mathbf{w}. \quad (12)$$

In contrast to \mathcal{P}_3 , the optimization problem \mathcal{P}_4 can be easily rewritten as a quadratic program (QP) in \mathbf{w} ; a widely studied type of program that facilitates the usage of power method-like iterations, and thus employing different signal constraints Ω —more on this later. In the following, we propose an efficient iterative optimization framework based on a separate optimization of the objective of \mathcal{P}_4 over its three partition of variables at each iteration, viz. \mathbf{w} , $\{\mathbf{Q}_i\}$, and $\{\lambda_i\}$, where the iterations can be started from any arbitrary initialization.

2.1. Power Method-Like Iterations (Optimization w. r. t. \mathbf{w})

For fixed $\{\mathbf{Q}_i\}$ and $\{\lambda_i\}$, one can optimize \mathcal{P}_4 w. r. t. \mathbf{w} via minimizing the criterion:

$$\sum_{i=1}^K \|\mathbf{A}_i^{\frac{1}{2}} \mathbf{w} - \sqrt{\lambda_i} \mathbf{Q}_i \mathbf{B}_i^{\frac{1}{2}} \mathbf{w}\|_2^2 = \mathbf{w}^H \mathbf{R} \mathbf{w} \quad (13)$$

where

$$\mathbf{R} = \sum_{i=1}^K \left\{ (\mathbf{A}_i + \lambda_i \mathbf{B}_i) - \sqrt{\lambda_i} (\mathbf{A}_i^{\frac{1}{2}} \mathbf{Q}_i \mathbf{B}_i^{\frac{1}{2}} + \mathbf{B}_i^{\frac{1}{2}} \mathbf{Q}_i^H \mathbf{A}_i^{\frac{1}{2}}) \right\}.$$

Due to the fact that Ω enforces a fixed ℓ_2 -norm on \mathbf{w} (i.e. $\|\mathbf{w}\|_2^2 = P$), by defining the PD matrix $\hat{\mathbf{R}} \triangleq \mu \mathbf{I} - \mathbf{R}$ (with $\mu > 0$ being larger than the maximum eigenvalue of \mathbf{R}), we have that $\mathbf{w}^H \mathbf{R} \mathbf{w} = -\mathbf{w}^H \hat{\mathbf{R}} \mathbf{w} + \mu P$ in which μP is constant. Consequently, one can minimize (or decrease monotonically) the criterion in (13) by maximizing (or increasing monotonically) the objective of the following optimization problem:

$$\max_{\mathbf{w}} \quad \mathbf{w}^H \hat{\mathbf{R}} \mathbf{w} \quad (14) \\ \text{s. t.} \quad \mathbf{w} \in \Omega.$$

Although (14) is NP-hard for a general signal constraint set [15, 16], a monotonically increasing objective of (14) can be obtained using *power method-like* iterations developed in [16], and [17]; namely, we update \mathbf{w} iteratively by solving the following *nearest-vector* problem at each iteration:

$$\min_{\mathbf{w}^{(s+1)}} \quad \left\| \mathbf{w}^{(s+1)} - \hat{\mathbf{R}} \mathbf{w}^{(s)} \right\|_2 \quad (15) \\ \text{s. t.} \quad \mathbf{w}^{(s+1)} \in \Omega,$$

where s denotes the internal iteration number, and $\mathbf{w}^{(0)}$ is the current value of \mathbf{w} . Note that we can continue updating \mathbf{w} until convergence in the objective of (14), or for a fixed number of steps, say S .

Now, we take a deeper look at various signal constraints Ω typically used in practice, as well as their associated constrained solutions to (15):

- *Total-power constraint:* In this case, Ω can be defined as $\Omega = \{\mathbf{w} : \|\mathbf{w}\|_2^2 = P\}$, where $P > 0$. Then, the set of power method-like iterations in (15) boils down to a typical power method aiming to find the dominant eigenvector of $\hat{\mathbf{R}}$, however with an additional scaling to attain a power of P .
- *Per-antenna power constraint:* We consider M antennas with assigned power values $\{P_i\}$, and assume that $K = N/M$ entries of \mathbf{w} are devoted to each antenna. As a result, we can solve (15) by considering the nearest-vector problem for sub-vectors associated with each antenna separately—i.e., M nearest-vector problems all with vector arguments of length K .
- *Unimodular signal design:* The set of unimodular codes is defined as $\Omega = \{e^{j\varphi} : \varphi \in [0, 2\pi)\}^N$. The unimodular solution to (15) is simply given by ($P = N$):

$$\mathbf{w}^{(s+1)} = \exp \left(j \arg \left(\hat{\mathbf{R}} \mathbf{w}^{(s)} \right) \right). \quad (16)$$

- *Discrete-phase signal design:* We define the set of discrete-phase signals as, $\Omega = \left\{ e^{j \frac{2\pi}{Q} q} : q = 0, 1, \dots, Q-1 \right\}^N$ where Q denotes the phase *quantization* level. The discrete-phase solution to (15) is given by ($P = N$):

$$\mathbf{w}^{(s+1)} = \exp \left(j \mu_Q \left(\arg \left(\hat{\mathbf{R}} \mathbf{w}^{(s)} \right) \right) \right) \quad (17)$$

where $\mu_Q(\cdot)$ yields (for each entry of the vector argument) the closest element in the Q -ary alphabet.

Finally, we refer the interested reader to find more details on the properties of power method-like iterations in [16]- [18].

2.2. Rotation-Aided Fitting (Optimization w. r. t. $\{\mathbf{Q}_i\}$)

Suppose \mathbf{w} and $\{\lambda_i\}$ are fixed. As discussed earlier, the maximizer \mathbf{Q}_i of \mathcal{P}_4 is a rotation matrix that maps $\mathbf{B}_i^{\frac{1}{2}}\mathbf{w}$ in the same direction as $\mathbf{A}_i^{\frac{1}{2}}\mathbf{w}$. Let

$$\begin{cases} \mathbf{u}_i = \mathbf{A}_i^{\frac{1}{2}}\mathbf{w} / \|\mathbf{A}_i^{\frac{1}{2}}\mathbf{w}\|_2, \\ \mathbf{v}_i = \mathbf{B}_i^{\frac{1}{2}}\mathbf{w} / \|\mathbf{B}_i^{\frac{1}{2}}\mathbf{w}\|_2, \end{cases} \quad (18)$$

and note that (12) can be rewritten as $\mathbf{u}_i = \mathbf{Q}_i\mathbf{v}_i$ for all $i \in [K]$. We define the unitary matrices $\mathbf{Q}_{\mathbf{u}_i}$ and $\mathbf{Q}_{\mathbf{v}_i}$ in $\mathbb{C}^{N \times N}$ as

$$\mathbf{Q}_{\mathbf{u}_i} = [\hat{\mathbf{u}}_{i1}, \hat{\mathbf{u}}_{i2}, \dots, \hat{\mathbf{u}}_{iN}] \quad (19)$$

$$\mathbf{Q}_{\mathbf{v}_i} = [\hat{\mathbf{v}}_{i1}, \hat{\mathbf{v}}_{i2}, \dots, \hat{\mathbf{v}}_{iN}] \quad (20)$$

where each of the sets $\{\hat{\mathbf{u}}_{ij}\}_j$ and $\{\hat{\mathbf{v}}_{ij}\}_j$, $j \in [N]$, builds an orthonormal basis for \mathbb{C}^N , and $\hat{\mathbf{u}}_{i1} = \mathbf{u}_i$, $\hat{\mathbf{v}}_{i1} = \mathbf{v}_i$. Based on the above definitions, the following lemma constructs the optimal \mathbf{Q}_i (the proof of Lemma 1 is straightforward and omitted herein):

Lemma 1. *The maximizer $\{\mathbf{Q}_i\}$ of \mathcal{P}_4 can be found as $\mathbf{Q}_i = \mathbf{Q}_{\mathbf{u}_i}\mathbf{Q}_{\mathbf{v}_i}^H$ for all $i \in [K]$.*

Remark 2: Note that $\{\mathbf{Q}_{\mathbf{u}_i}\}$ and $\{\mathbf{Q}_{\mathbf{v}_i}\}$ can be obtained via the Gram-Schmidt process, and are not generally unique since $\{\hat{\mathbf{u}}_{ij}\}$ and $\{\hat{\mathbf{v}}_{ij}\}$ can be chosen rather arbitrarily for $j \neq 1$. This further implies that the maximizer $\{\mathbf{Q}_i\}$ of \mathcal{P}_4 is also not unique, which is in agreement with the common understanding that rotation matrices are not necessarily unique when the dimension grows large. ■

2.3. Grab-n-Pull (Optimization w. r. t. $\{\lambda_i\}$)

Note that, once the optimal $\{\mathbf{Q}_i\}$ is used, the objectives of \mathcal{P}_3 and \mathcal{P}_4 can be considered interchangeably. We assume that the optimal \mathbf{w} and $\{\mathbf{Q}_i\}$ are obtained according to the above discussions, and are fixed. Therefore, to find $\{\lambda_i\}$, we can equivalently focus on obtaining the maximizer $\{\lambda_i\}$ of \mathcal{P}_3 via the optimization problem:

$$\begin{aligned} \Lambda : \quad & \max_{\{\lambda_i\}} \min_{i \in [K]} \{\lambda_i\} - \eta \sum_{i=1}^K (\|\mathbf{A}_i^{\frac{1}{2}}\mathbf{w}\|_2 - \sqrt{\lambda_i}\|\mathbf{B}_i^{\frac{1}{2}}\mathbf{w}\|_2)^2 \\ \text{s. t.} \quad & \lambda_i \geq 0, \forall i \in [K]. \end{aligned} \quad (21)$$

Definition 1. *Let $\{\lambda_i^*\}$ denote the optimal $\{\lambda_i\}$ of Λ , and $\lambda^* \triangleq \min_{i \in [K]} \{\lambda_i^*\}$. We let Υ to denote the set of all indices m for which λ_m^* takes the minimal value among all $\{\lambda_i^*\}$, i.e.*

$$\Upsilon = \{m \in [K] : \lambda_m^* = \lambda^*\}. \quad (22)$$

Moreover, we refer to $\gamma_i^2 \triangleq \|\mathbf{A}_i^{\frac{1}{2}}\mathbf{w}\|_2^2 / \|\mathbf{B}_i^{\frac{1}{2}}\mathbf{w}\|_2^2$ as the *shadow value* of λ_i^* , for all $i \in [K]$.

It is straightforward to verify from the objective of Λ that if $\lambda_i^* > \lambda^*$, then $\lambda_i^* = \gamma_i^2$. On the other hand, to obtain λ^* , we need to maximize the criterion:

$$f(\lambda) = \lambda - \eta \sum_{k \in \Upsilon} \left(\|\mathbf{A}_k^{\frac{1}{2}}\mathbf{w}\|_2 - \sqrt{\lambda}\|\mathbf{B}_k^{\frac{1}{2}}\mathbf{w}\|_2 \right)^2. \quad (23)$$

Provided that η is large enough (see the lower bound in Theorem 1), the optimal λ^* of the above quadratic criterion (in $\sqrt{\lambda}$) is given by

$$\sqrt{\lambda^*} = \frac{\eta \sum_{k \in \Upsilon} \alpha_k \beta_k}{\eta \sum_{k \in \Upsilon} \beta_k^2 - 1} \quad (24)$$

in which $\alpha_k \triangleq \|\mathbf{A}_k^{\frac{1}{2}}\mathbf{w}\|_2$, and $\beta_k \triangleq \|\mathbf{B}_k^{\frac{1}{2}}\mathbf{w}\|_2$. It is interesting to have some insight into what $\sqrt{\lambda^*}$ represents: Note that (24) can be rewritten as

$$\sqrt{\lambda^*} = \frac{\sum_{k \in \Upsilon} \gamma_k \beta_k^2}{\sum_{k \in \Upsilon} \beta_k^2 - 1/\eta}. \quad (25)$$

As a result, $\sqrt{\lambda^*}$ can be viewed as a weighted average of γ_k for $k \in \Upsilon$ —except that the term $-1/\eta$ in the denominator of (25) makes $\sqrt{\lambda^*}$ a bit larger than the actual weighted average. However, for an increasing η , $\sqrt{\lambda^*}$ converges to the exact value of the weighted average specified above.

Hereafter, we propose a recursive *Grab-n-Pull* procedure to fully determine Υ , while we can obtain $\sqrt{\lambda^*}$ via (24). The proposed approach will make use of the following observation:

Lemma 2. *If $\gamma_i^2 < \lambda^*$ for any $i \in [K]$, then $i \in \Upsilon$.*

Proof. The inequality $\gamma_i^2 < \lambda^*$ implies that $\lambda_i^* \neq \gamma_i^2$. Considering the discussion above (23), one can conclude that $\lambda_i^* \leq \lambda^*$, which due to the definition of λ^* yields $\lambda_i^* = \lambda^*$. Hence, the proof is complete. □

Without loss of generality, and for the sake of simplicity, we assume in the sequel that the matrix pairs $\{(\mathbf{A}_i, \mathbf{B}_i)\}$ are sorted in such a way to form the ascending order:

$$0 \leq \gamma_1 \leq \gamma_2 \leq \dots \leq \gamma_K. \quad (26)$$

Based on the above ordering, the Grab-n-Pull approach is described in Table 1. Moreover, an illustration of the method is depicted in Fig. 1. The name of the method, i.e. Grab-n-Pull, comes from the intuition that the method *grabs* and *pulls* the lowest values of $\{\lambda_i\}$ to a level which is suitable for optimization of the alternative objectives, while achieving *equality*, at least for the *lowest* λ_i s. Due to the key role of Grab-n-Pull procedure in the proposed optimization framework, we also use the term Grab-n-Pull when referring to the general framework. In the following, we present a specific criterion on η that not only bounds the objective of \mathcal{P}_4 (and \mathcal{P}_3), but also guarantees the convergence of the proposed approach.

Theorem 1. *Suppose η is chosen such that*

$$\eta > \eta_b \triangleq \frac{1}{P} \left(\max_{i \in [K]} \{\sigma_{\min}^{-1}(\mathbf{B}_k)\} \right). \quad (27)$$

Then, $f(\lambda)$ is upper bounded (at its maximizer λ^* , see (24)) as

$$\begin{aligned} f(\lambda^*) & \leq \frac{\sum_{k \in \Upsilon} \alpha_k^2}{\sum_{k \in \Upsilon} \beta_k^2 - 1/\eta} \\ & \leq \sigma_{\max} \left\{ \left(\left(\sum_{k \in \Upsilon} \mathbf{B}_k \right) - \frac{1}{\eta P} \mathbf{I} \right)^{-1} \left(\sum_{k \in \Upsilon} \mathbf{A}_k \right) \right\}. \end{aligned} \quad (28)$$

The proof of Theorem 1 is omitted herein due to lack of space. Nevertheless, to see why the latter result implies the convergence of our algorithm, one can observe that different steps of the proposed framework lead to an increasing objective of \mathcal{P}_4 (and \mathcal{P}_3). To guarantee convergence in terms of the objective value, we only need to show that the objective is bounded from above—a condition which will be met by satisfying (27).

Table 1. Recursive Grab-n-Pull Procedure to Determine Υ

Step 0: Set $\Upsilon = \emptyset$.

Step 1: Include 1 in Υ .

Remark: Based on Lemma 2, the primitive index 1 belongs to Υ , as $\sqrt{\lambda^*}$ is always larger than γ_1 .

Step 2: Given the current index set of minimal variables Υ , obtain $\sqrt{\lambda^*}$ using (24).

Remark: Note that if $\sqrt{\lambda^*}$ is smaller than γ_k for all $k \in [K] \setminus \Upsilon$ then the obtained Υ is optimal, as all λ_k with $k \in [K] \setminus \Upsilon$ have chosen their values freely to maximize the objective of Λ ; as a result, adding other indices to Υ will lead to a decreased objective of Λ .

Step 3: Let $\{h\} \subset [K]$ denote the indices for which $h \notin \Upsilon$. If $\gamma_h \leq \sqrt{\lambda^*}$, include h in Υ , and goto Step 2; otherwise stop.

Remark: This is a direct consequence of Lemma 2, particularly considering that $\sqrt{\lambda^*}$ is only increasing with growing $|\Upsilon|$, which corresponds to adding larger γ_i s to the weighted sum in (25).

3. A NUMERICAL EXAMPLE WITH DISCUSSIONS

In this section, a brief numerical example is provided to investigate the performance of the proposed method (performing the optimization w. r. t. to all variables at each iteration). To this end, we consider a downlink transmitter with $M = 4$ antennas, as well as $K = 4$ single-antenna users. The entries of the channel vectors \mathbf{h}_i are drawn from an i.i.d. complex Gaussian distribution with zero-mean and unit-variance. The Gaussian noise components received at each user antenna are assumed to have unit variance, i.e. $\sigma_i^2 = 1$ for all $i \in [K]$. We consider a total-power constraint with $P = 1$, and stop the optimization iterations whenever the objective increase becomes bounded by $\epsilon = 10^{-6}$.

Note that while the shadow values $\{\gamma_i^2\}$ represent the value of the fractional quadratic terms in the original objective \mathcal{P}_1 , the auxiliary variables $\{\lambda_i\}$ tend to be as close as possible to $\{\gamma_i^2\}$ depending on the weight (η) of the penalty-terms in \mathcal{P}_3 and \mathcal{P}_4 . In Fig. 2, we present the transition of variables $\{\gamma_i^2\}$ and $\{\lambda_i\}$ vs. the iteration number for two different settings of η ; namely $\eta = 5$ and $\eta = 100$. Although with a larger η one may expect a lower value of the penalty functions in \mathcal{P}_3 and \mathcal{P}_4 , a lower η can play a useful role in speeding up the algorithm. Specifically, one can easily see that if η is large, the value λ^* in (25) will be slightly greater than the weighted average of $\{\gamma_k^2\}_{k \in \Upsilon}$, whereas for smaller values of η , the bounces from the weighted average are much larger—and the convergence can occur much quicker. This phenomenon can also be observed in Fig. 2., noting that the aforementioned values of η are chosen to accentuate the trade-off originated from the selection of η .

It should be mentioned that for the special case of the total-power constraint, all optimal $\{\lambda_i\}$ are shown to be identical [1], i.e. $\lambda_i = \lambda^*$ for all $i \in [K]$. This explains the identical values obtained by the method in Fig. 2. The results leading to Fig. 2 were obtained in a few seconds on a standard PC.

4. CONCLUSION

An optimization framework for efficient precoding/beamforming in fairness-achieving networks was proposed. Thanks to a quadratic reformulation of the original problem, the proposed method can handle different signal constraints by employing the power method-like iterations. Various aspects of the proposed approach were studied.

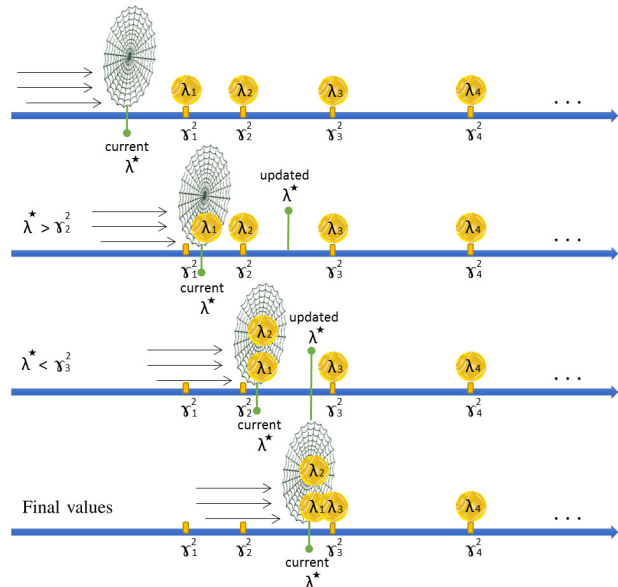


Fig. 1. An illustration of the Grab-n-Pull procedure. The optimal values of $\{\lambda_i\}$ are obtained when $\lambda^* < \gamma_3^2$, which sets Υ to $\{1, 2\}$.

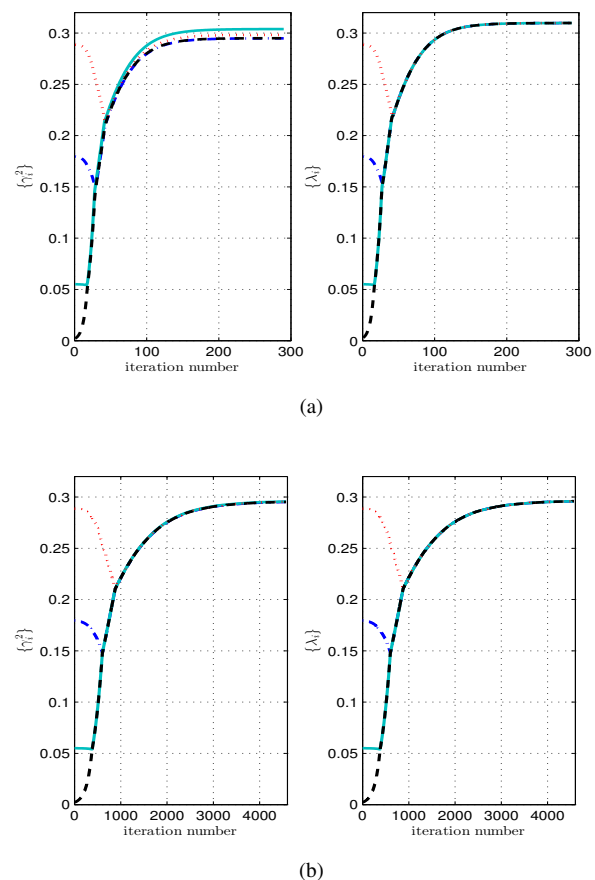


Fig. 2. Transition of the optimization parameters (distinguished by colors and line-styles) vs. the iteration number for different weights (η) of the penalty-term in \mathcal{P}_3 and \mathcal{P}_4 : (a) $\eta = 5$, and (b) $\eta = 100$.

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